Date of publication xxxx 00, 0000, date of current version xxxx 00, 0000.

Digital Object Identifier 10.1109/ACCESS.2017.Doi Number

Antenna for Ultra-Wideband Applications with Non-Uniform Defected Ground Plane and Offset Aperture-Coupled Cylindrical Dielectric Resonators

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This work was supported in part by the Innovation Programme under Grant H2020-MSCA-ITN-2016 SECRET-722424 and in part by the U.K. Engineering and Physical Sciences Research Council (EPSRC) under Grant EP/E022936/1.

ABSTRACT A new compact Cylindrical Dielectric Resonator Antenna (CDRA) with a defected ground for ultra-wideband applications is presented. The structure is based on two cylindrical dielectric resonators asymmetrically located with respect to the center of an offset rectangular coupling aperture, with consideration of three and four Dielectric Resonators (DR). The resonant modes generated by the defected ground are studied and investigated. A parametric optimization study of the antenna design has been carried out to determine the optimal dimensions of the defected ground plane, resulting in an impedance bandwidth of over 133% that covers the frequency band from 3.6 GHz to 18.0 GHz. A power gain of about 7.9 dBi has been achieved. Design details and measured and simulated results are presented and discussed.

INDEX TERMS Cylindrical Dielectric Resonators Antenna, Ultra-Wideband, Defected Ground Structure.

I. INTRODUCTION

Recently, the Defected Ground Structure (DGS) technique has received much attention in the design of microwave and millimeter wave sub-systems. It consists of etching variously shaped apertures in the ground plane to create a disturbance in the current distribution [1], [2]. For more than a decade, frequency-selective properties of DGSs have been widely used in printed circuits and antenna applications. DGS were first proposed for antenna applications in 2005 [3]. Among other benefits, the technique can reduce cross-polarization, which constitutes a major drawback for some wideband antennas [4].

In recent studies, the DGS technique is mainly employed to improve the impedance bandwidth of patch antenna structures [1]. Similar topics were treated in [2], [4], [5]. This technique can also be used to reduce coupling [6], minimize the structure size, and excite additional resonance modes using simple and compact DGSs configurations [7], [8]. It can be used to achieve single-feed multi-frequency microstrip antennas, including multiband functions using various DGSs [9], [10]. Moreover, the use of DGS can also enhance the antenna gain [2], [11], [12]. In this context, DGSs of many shapes have been investigated, such as circles, spirals, concentric rings, elliptical dumbbells and U and V slots [2]-[4]. Shapes such as rectangular, square, or semi-circular arcs [1] with varying dimensions can provide particular improvements in DGS-based antenna performances [4]. DGS has been used in controlling active microstrip antennas [4]. In [13] and [14], DGSs were used to design desired dual and triple band-notched UWB antennas. In [15], a shovel-shaped DGS was used in a simple and compact UWB planar monopole antenna with filtering characteristics. In [16], a simple CPW-fed monopole patch antenna surrounded with a coplanar ground plane was presented. Further modifications of the DGS was made to enhance the gain and impedance bandwidth [16]. This technique was extended to Dielectric Resonator Antennas (DRAs), where the mutual coupling between two circular microstrip patches was suppressed making use of the stop-band property of the proposed DGS.

DRAs have emerged as a novel radiation technology, with the advantage of having high efficiency. Consequently, special DRA shapes and multi-segment DRAs have been reviewed extensively. Rectangular [17], Conical [18], asymmetrical E [19], Stair-Shaped [20], Inverted L-shaped [21], elliptical [22], asymmetrical T-shaped [23], tetrahedral [24] with triangular slot [25], ring-shaped [4] cylindrical [2][26]-[28], and hybrid hemispherical-conical-shaped [29] configurations have all been suggested for antenna bandwidth enhancement. Gain and bandwidth enhancement configurations were presented in [2] and [30], where two cylindrical dielectric resonators were asymmetrically placed around the center of the rectangular coupling aperture, and fed through this defected ground plane aperture. In [30], a parametric optimization study was carried out and a bandwidth of about 57% was achieved, covering 8.02 to 14.55 GHz with a 10 dBi power gain. These results are quite comparable to those found in [2], namely a bandwidth of about 54%, a frequency band from 8.5 to 14.7 GHz and a 12 dBi gain.

Currently, the operating bandwidth of antennas using DRAs has been further improved for ultra-wideband applications [29], [30], [31]. In [32], a mono-cylindrical Dielectric Resonator (DR) was fed using two crossed slots centered at different locations. The slot modes were considered partially independent from the DR mode; in consequence, a wide bandwidth is attained. In [2], [26] and [30], wideband slot-fed asymmetric DRAs analyses were presented, where two adjacent cylindrical dielectric resonators were placed asymmetrically around the rectangular feeding aperture. The asymmetrical locations provide a further optimization parameter in the DRA design. As a result, the proposed antenna parameters are significantly improved: a 29% impedance bandwidth, a 9.62 to 12.9 GHz frequency band and an 8 dBi realized gain were achieved [26].

The present paper extends our recent work [27], which presented a compact ultra-wideband DRA using two cylindrical dielectric resonators asymmetrically placed near the center of an offset rectangular coupling aperture; this resulted in a 62% bandwidth, covering the two bands 5.9 to 7.32 GHz and 8.72 to 16.57 GHz, with a gain of 8 dBi. Herein, using the same aperture concept, the relative bandwidth is increased up to 133.33% covering the range from 3.6 to 18 GHz. This range covers C band (4 to 8 GHz), X band (8 to 12.4 GHz) and Ku band (12.4 to 18 GHz), comprising services such as earth-to-satellite bands at 5.9 to 6.4 GHz, 12.25 to 13.25 GHz and 14 to 14.5 GHz, connections for satellite-earth at 10.7 to 11.7 GHz, 10.5 GHz for police radar and, for commercial use, 10.7 to 13.2 GHz.

The current basic design is a defected ground plane microstrip-fed DRA obtained by modifying the initial design in [27] (Figure 2.a (i))achieving further enhancements in impedance bandwidth and gain. Experimental and simulation results of the resulting novel antenna are presented and discussed. The present work mainly intended to improve our recently published work [27], where the bandwidth is improved twice by use of DGS technique. The novelty of this work, hence, lies in the combination of the DGS with the DRA structures.

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| --- |
|  |
| **(a)** |
|  |
| **(b)** |

FIGURE 1.  Design parameters of two aperture-coupled DRAs with non-uniform defected ground plane, (a) top view and (b) side view.

II. PROPOSED ANTENNA GEOMETRY AND SUMMARIZED RESULTS

The geometry of the basic monopole antenna design is shown in Figure 1. A microstrip feed is used due to its impedance matching simplicity and other useful features [27]. The proposed asymmetric ultra-wideband antenna with a defected ground plane is designed and realized on an FR4 30×25×0.8 mm3 substrate with relative permittivity *εrs*=4.4 and 0.017 loss tangent. Two identical alumina-96%-DRs of radius *D* =6 mm and height *h* =9 mm have been used. A feeding microstrip line of length *lf* =20.5 mm and width *wf*=1.5 mm is located symmetrically around the coupling aperture. Its dimensions were calculated using empirical formulas [2], [26], [27], [30], [32].

Simulations for this geometry were carried out using HFSS software. Two identical rectangular apertures (slots) of length *ls* and width *ws* are etched on the ground plane, shifted from the center by a distance *d*. Based on the experimental results obtained in [27], a stub length close to λg/4 is also used in this design, although this differs from that of [27] by including the ground plane apertures. The final antenna dimensions (Figure 1) *wf*=1.5 mm, *lf*=20.5 mm, *ws*=3.5 mm, *ls*=6.6 mm, *ds* =3.1 mm and *d*=0.2 mm are optimized in our previous work [27], and the dimensions of the defected antenna are *wg*=16.25 mm, *lg*=16.5 mm, *x1*=6.5 mm, *x2*=13.5 mm, *x3*=1.5 mm, *y1*=8.75 mm, *y2*=8.75 mm and *y3* =3.15 mm.

III. CHARACTERISTIC MODES DESCRIPTIONS

Building on previous works [2], [26], [30], [27], modifications are applied to the basic antenna according to the realization steps of our model shown in Figure 2 (a). The originality of this work lies in the creation of a defected ground plane for exciting further modes [2] and enhancing the bandwidth and gain. The segmentation of the ground plane improves the return loss S11 as illustrated in Fig.2 (b).

As shown in Table I, all four proposed designs (ii) to (v), presented in Figure 2 (a), have a bandwidth greater than that of antenna (i) presented in [27]. The application of the DGS technique has led to a single band extending from 3.6 to 18 GHz, i.e. a 133.33 % relative bandwidth. It should be noted that the major improvement achieved by this technique occurs below 10 GHz (3.6-10 GHz). The introduction of the defected ground to the slotted structure (Antenna (i) [27]) led to the appearance of other resonance frequencies between 3.6 and 6 GHz, and from 6 to 10 GHz due to the combined effect of the DRA and the slotted defected ground.

TABLE I

Bandwidth of the five designs shown in Figure (2.a).

|  |  |  |
| --- | --- | --- |
| Design | BW (GHz) | BW (%) |
| i[27] | 5.9-7.4 and 9.1-17.8 | 22.56 and 64.68 |
| ii | 5.5-7.3 and 9-17.8 | 28.13 and 65.67 |
| iii | 5.6-7.6 and 8.3-17.8 | 30.30 and 72.79 |
| iv | 3.7-17.9 | 131.48 |
| Prototype | 3.6-18 | 133.33 |

Although the existing literature clearly favors probe excitation at lower frequencies where coupling apertures are not often used due to their large size [33], [34], in our case, large slots, when combined with the DGS technique, has shown better excitation performances for a two DR structure. This combination is considered as the main novelty of this work.

Generally, isolated cylindrical DRAs support TE, TM and hybrid resonant modes [28], [35], [36], in a widely adopted designation. Amongst multiple cylindrical DRA modes, the TE01δ, TM01δ, and hybrid HEM11δ (with dominant Ez component) modes are the most commonly considered radiating modes. The subscript numbers in the mode designation express the field variation in the azimuth, radial and axial directions, respectively. The index δ, lying between 0 and 1, indicates the resonant behavior along the dielectric cylinder height (z axis). The TE01δ mode, TM01δ mode and HEM11δ mode radiate similarly to the short vertical magnetic dipole, short vertical electric dipole and short horizontal magnetic dipole, respectively [36].

In our case, a large double slot is etched in the ground plane, resulting in multiple magnetic/electric modes over frequency. The slot has more effect depending on the frequency; it resonates at low frequencies exciting the DRA at 10 and 12, and up to 16 GHz, (Figure 2).

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| --- | --- | --- | --- |
|  |  | |  |
| **i** | **ii** | | **iii** |
|  | |  | |
| **iv** | | **v** | |
| **(a)** | | | |
|  | | | |
| **(b)** | | | |

FIGURE 2.  (a) Evolution of the proposed antenna, (i) the design of [27], (ii), (iii),(iv), (v) steps of design optimization. (b) simulated S11 of the five designs shown in (a).

Much research has focused on cylindrical DRAs [28], [37]-[40]. In [38] and [39], the DRA device is used as sensors for wireless networks and liquid chemical detection applications, respectively. In these structures, the TM and quasi-TM modes can be excited by placing the dielectric disk on the ground plane [41]. Little attention has been paid to the TE and quasi-TE modes, which cannot be excited when the base of the DRA is placed on the ground plane [42]. In [42], some DRA HEM11*δ* and HEM12*δ* mode features, compared to the most widely studied TM01*δ* and TE01*δ* modes, are briefly discussed. The resonant frequency *fo* of the TE01*δ* mode, TM01*δ* mode, and HEM11*δ* are respectively given by the following empirical equations [36], [43], [44]:

 (1)

 (2)

 (3)

where *ε*r is the DR relative permittivity, *a* is the radius and *h* is the height of the dielectric cylinder. Note that there are neither exact mathematical expressions for the resonant frequencies of higher order modes nor exact solutions for their internal fields and radiation patterns [36]. An approximate solution for the cylindrical DRAs field pattern has been obtained by considering a magnetic wall boundary condition on the surfaces parallel to the *z* axis [45].

The slot length is calculated using the following [44]:

 (4)

where *εr* and *εrs* are the relative dielectric constant of the DR and substrate, respectively. In [46], measurements of the cylindrical dielectric resonator HEM11δ mode radiation efficiency for *εr* = 38 show values better than 98%.

The slot in our case (with wide zigzag) has changed the shape of the magnetic current (magnetic dipole), and excited other modes at low frequencies (less than 10 GHz) (Figure 2 (b)). The equations (1-7) of the resonant frequency modes were derived from the calculations of the cylindrical dielectric resonator by considering perfect electric and/or magnetic walls on the resonator faces. The perfect magnetic wall condition was shown to be accurate for higher *εr* values [47], but remains fairly valid for lower values.

The three first modeTE01*δ*, TM01*δ,* and HEM11*δ* resonant frequencies of the cylindrical resonator are given by the following empirical expressions [33]:

 (5)



 (6)

 (7)

where *a* and *h* are respectively the DR radius and height.

The differences between these equations are clarified by an example in Table II, as these equations do not include any information about the coupling factor or the quality factor of CDRA and the approximation is given with respect to ratio (*a/h*).

The DRA resonant frequency can be controlled by varying the length of the slot, which may also help in reconfiguring the radiation patterns.

When a single shaped DRA operates in the fundamental mode, its bandwidth typically does not exceed 10% [48]. Experimental work on wide-band DRAs was described in 1989 by Kishk *et al.* [48] who proposed using two separate DRAs stacked end to end to achieve a dual-resonance band. Other wideband configurations using this technique have since been reported [49]-[51].

An alumina-96% based DRA (*εr* = 9.4) has been designed with a diameter *D* = 6 mm and a height *h* = 9mm. The resonant frequency of a single segment CDRA excited in HEM11δ mode is given by [26], [27]

 (8)

where *a = D/2* (in cm), *c* is the free space light velocity. For these dimensions, the calculated frequency is 10.63 GHz. The DRs are asymmetrically placed around the asymmetrical slots, hence, the DRA modes depend on the DR geometrical parameters, the permittivity and the feeding mechanism. The asymmetric DR pair configuration and the dimensions and shape of the defected ground give designers more scope for functional optimization. In this study, a 133% impedance bandwidth, covering 3.6 GHz to 18.0 GHz, has been achieved.

Table II compares the results of the 7 equations mentioned above for *a* = 3 mm, *h* = 9 mm and *εr* = 9.4. The resonant frequencies of dielectric resonators are determined using rigorous numerical methods [43].

According to *εr* and *a/h*, closed-form expressions for different modes are obtained. The accuracy of the formulas presented above (Equations 1-8) is demonstrated for the same resonator parameters for which the results of rigorous numerical methods available in the literature are very close [43].

TABLE II

Bandwidth of the five designs shown in Figure (2.a).

|  |  |  |
| --- | --- | --- |
| Design | BW (GHz) | BW (%) |
| Equ (1)/TE | 1.2285e+10 | 0.3177 |
| Equ (5)/TE | 1.2437e+10 |
| Equ (2)/ TM | 1.8222e+10 | 1.2171 |
| Equ (6)/TM | 1.8193e+10 |
| Equ (3)/ HEM | 9.9366e+09 | 6.0101 |
| Equ (7)/ HEM | 1.0484e+10 |
| Equ (7)/ HEM | 1.0484e+10 | 1.3728 |
| Equ (8)/HEM | 1.0630e+10 |

Let us conclude this part with a comparison of the size of our antenna with those realized or simulated available in the literature.

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| **(a)** | |
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| **(b)** | |
|  |  |
| **(c)** | |
|  |  |
| **(d)** | |
| FIGURE 3.  Effect of different slit lengths on S11 of the aperture-coupled asymmetric DRA with DGS, compared with the proposed antenna and with the antenna in [27]. (a) Effect of slit length x1 (y1=0mm) and the effect of the slit length y1 (x1=6.5mm), (b) Effect of the slit length x2 (x1=6.5mm and y1=y2=8.75mm), (c) Effect of the slit length y2 with x1=6.5mm, y1=8.75mm and x2=13.5mm, (d) Effect of the slit x3×y3with x1=6.5mm, y1=8.75mm and x2=13.5mm. | |

It is clear from Table III that our proposed structure presents a good compromise between miniaturization and the significant gain obtained compared to the reported studies.

TABLE III

Antenna dimensions and properties comparison with published data.

|  |  |  |  |
| --- | --- | --- | --- |
| Reference, Year | Total Area  (mm3) | Operating  bands(GHz) | Gain  dBi |
| [18], 2013 | 100×100×20 | 3.5-10.5 | 4.25-8.3 |
| [26], 2014 | 30×25×9.8 | 9.62-12.9 | 6-8 |
| [19], 2016 | 50×50×5.8 | 6.0–10.2 | 4.5-8.1 |
| [20], 2016 | 27×25×6.8 | 3.844-8.146 | 3-3.9 |
| [21], 2017 | 44×44×10.8 | 3.76-9.35 | 5-8 |
| [23], 2012 | 60×60×13.6 | 3.81 to 8.39 | 3-24-7.75 |
| [22], 2018 | 80×80×9 | 8.26 - 12.15 | 6.2-8.1 |
| [25], 2017 | 140×140×5.8 | 3.8–8.1 | 5.5 to 7.5 |
| [29], 2012 | 70×70×11 | 4-16 | 2–4 |
| [30], 2016 | 30×25×9.8 | 9.1-14.6 | 6.2-8 |
| [2], 2017 | 30×25×9.8 | 8.02-14.55 | 6-12 |
| [27], 2017 | 30×25×9.8 | 5.9-7.32/8.7-15 | 6-12 |
| [28], 2019 | 120×120×12 | 2.33-2.52 | 6.2 |
| Our proposed  antenna | 30×25×9.8 | 3.6-18 | 6-8 |

Figure 3a shows the ground plane length effect on the reflection coefficient. It is clearly seen that it acts most strongly on frequencies below 10 GHz. In this case, the optimal value for *x1* is 6.5 mm. The width of the second truncation (*y1)* is in the *y*-direction. It is noted that the effect is clearly visible in the frequency band 3-10 GHz. In this case, the impedance matching is better at *y1* = 8.75 mm, where the mismatch between 7 and 10 GHz decreases with respect to *y1* and is optimal for *y1* = 8.75 mm for frequencies beyond 10 GHz, which are less affected by the truncation of the ground plane.

Figure 3b shows that increasing *x2* up to 13.5 mm improves the bandwidth. Beyond 17 mm, a mismatch is observed for lower frequencies. From Figure 3c, we note that for *x2* = 13.5 mm with varying *y2*, a further bandwidth improvement is obtained for *y2=*8.75 mm. In Fig.3d, the effect of the truncation *x3×y3* is not clearly visible, but in reality, a slight increase of 1% in bandwidth for *x3*×*y3* =1.5mm×3.15mm is obtained.

To validate the simulated results, an antenna prototype is constructed as shown in Figure 4a, and its parameters were measured using a vector network analyzer. The measurement of the proposed antenna with and without DRs results are also compared and are in good agreement with the simulation ones.

Figure 4b shows good agreement between measurements and simulations of the antenna without DR. We can notice that this antenna works in the frequency bands 3.9-6GHz and 11.1-12.8GHZ only by the application of the DGS and the slot techniques without the introduction of the DR. Figures 4 (c) and (d) present the prototype of the antenna with DR and the simulated and measured S11 without and with consideration of the glue thickness, respectively. It is remarkable with confirmation that the glue has a considerable effect on S11, especially at high frequencies. In general, the obtained results are in good agreement.

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| **(a)** | |
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| **(b)** | |
|  | |
| **(c)** | |
|  | |
| **(d)** | |

FIGURE 4.  Proposed antenna. (a) antenna faces photograph without DR, (b) Measured and simulated reflection coefficient of the antenna without DR (c) our proposed antenna photograph with two DRs, (d) Measured and simulated reflection coefficient of the proposed antenna with DR (with glue of various thicknesses t)

Figures 5(a) and (b) show the benefit of the introduction of the cylindrical DR to excite more hybrid modes than with a rectangular DR, as was previously reported in [27].

According to [33], the frequencies of the three lowest modes HEM01δ, TE01δ and TM01δ of a single cylindrical DRA are 10.484, 12.188 and 18.164 GHz, respectively, while in [43], [53] the resonant frequencies for HE11δ, EH11δ, TE11δ and TM01δ modes are 9.8469, 10.2358, 12.2768 and 18.2089 GHz, respectively. These modes are only excited by a single DRA, so it is possible for other modes to be excited at low frequencies by the two DRAs (the same effect as for the rectangular DRA in [27]).

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| **(a)** |
|  |
| **(b)** |
| **FIGURE 5.** **(a) Simulated S11 of 2-cylindrical DRA compared to a single rectangular DRA with the same overall dimensions, (b) Simulated input impedance of 2-cylindrical DRA compared to a single rectangular DRA.** |
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| **FIGURE 6.**  **Magnitude of electric field distribution for 7.0 GHz and (TEδ11, quasi-HE11δ) 9.4 GHz, 10.5GHz (HEM01δ, EH11δ, TE1δ1, and TE11δ) 12.4 GHz (TE01δ), 16.0 GHz (TE102 and TEδ21) and 17.5 GHz (TM01δ).( xz plane, yz plane).** |

It should be noted that in this study, the ground plane used is defected while a full sized plane is used in [27].

The presented results give an additional proof to the equivalence between the two cylindrical DR's with a single rectangular DR having the same overall dimensions.

For the case of a single rectangular DR, according to [54] and [27], the frequencies of TEδ11, TE1δ1 and TE11δ modes are 7.19, 10.23 and 10.51 GHz, respectively. In total, the excited modes are TEδ11 at 7 GHz, HE11δ at 9.85 GHz, and around 10 GHz, we have excited modes (HEM01δ, EH11δ, TE1δ1, and TE11δ), as shown in Fig.6. The TE102 and TEδ21 modes are excited at 12.4 and 16 GHz [27], and finally the mode TM01δ at 17.5 GHz (Figure 6).

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| **FIGURE 7.** **Measured and simulated gains of the proposed antennas.** |

Figures 7 and 8 illustrate respectively the measured and simulated gains in the broadside direction and efficiency of the presented antenna. The simulated gain assumes an ideal feeding network, whereas the measurements include the actual feeding network insertion loss, hence there are local discrepancies. The plot shows the calculated gain varying between 4.30 and 9.98 dBi with a maximum of 9.98 dBi at 15GHz, while the measured gain varies between 5.65 and 7.9 dBi in the band from 6 to17.5GHz, with a maximum of 7.9 dBi at 17.5 GHz. Additionally, the measured radiation efficiencies are over 75 % from 3.6 to18 GHz.

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| **FIGURE 8.** **Measured and simulated efficiency of the proposed antenna.** |
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| **FIGURE 9.** **Measured radiation patterns of the proposed antenna. Left: xy-plane, middle: xz-plane and right: yz-plane.** | |

Figure 9 shows radiation patterns measured at frequencies 4.1, 7, 9.4, 10.5 and 17.5 GHz. This shows that the antenna has a wide radiation pattern with a maximum along the normal to the substrate, covering a half-space. In some cases, an almost omnidirectional radiation pattern is observed.

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| **FIGURE 10.** Simulated and measured group delay of the proposed antenna. |

Form Figure10, the antenna provides linear S21 response and non-varying group delay response in the 3.6-18GHz, where a maximum and minimum values of simulated group delay respectively is 1.19 and 0.7 ns whereas the measured is 1.19 and 0.66 ns, which shows an acceptable performance in time-domain.

|  |
| --- |
| **20151019_143112** |
| **(a)** |
|  |
| **(b)** |
| **FIGURE 11. (a) Proposed antenna with three DRs (1st configuration).**  **(b) Simulated and measured S11 of 3-DR antenna.** |

IV. EFFECT OF DRs NUMBER

The proposed arrangement of two slots feeding the two DRs gives an extra degree of freedom in the design procedure. The achieved higher bandwidth can be interpreted as the result of merging many resonating frequencies bands of the different parts constituting the antenna. Obviously, adding a second slot has resulted in increased bandwidth. Wherever each resonant frequency can be attributed to a relevant part of the antenna, the designer will have a wider scope to tailor the required extension of the bandwidth.

While the resonating parts of the antenna: DRs, slots and feed line/stub are the most influential factors on the antenna characteristics, the effect of the DR number with a wide slot on S11 is also investigated.

The DR number effect is very important compared to the slot, as is well illustrated by Figures 11, 12 and 13.

For the first case (3-DR antenna configuration), we could theoretically have a bandwidth of 3.4-8.05 and 9.25-16.85GHz and experimentally 3.35-13.45 and 14.45-16.5GHz (Fig. 11).

In the second configuration, the bandwidth is shifted to 3.05-7.85GHz and 9.15-12.3GHz; a slight variation between the theoretical and the experimental results is observed (Fig. 12).

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| **20151019_143718** |
| **(a)** |
|  |
| **(b)** |
| **FIGURE 12. (a) Proposed antenna with three DRs (2nd configuration)**  **(b) Simulated and measured S11 of 3-DR antenna.** |

For the third case (4-DR antenna configuration, Fig.13), the frequency is shifted down to 3GHz; but in this case the antenna bandwidth becomes relatively narrower.

The advantage of having a wide slot is to excite the lower frequencies and this can, with an adequate number of DRs, control the usable frequency band.

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| **(a)** |
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| **(b)** |
| **FIGURE 13.(a) Proposed antenna with four DRs (3nd configuration)**  **(b)Simulated and measured S11 of 4-DR antenna.** |

V. CONCLUSION

In this work, a compact dielectric resonator antenna for ultra-wideband applications has been studied. It has been shown that the use of dielectric resonators enhances the antenna performance. The asymmetric placement of the DR pair (three and four), the defected ground technique, the dimensions and the shape of the aperture together give designers more scope for the optimization process. More resonances can be generated and the bandwidth has thereby been improved. The obtained results show that an impedance bandwidth of 133.33%, covering the UWB 3.6 GHz to 18.0 GHz, and a maximum simulated and measured power gain of 9.9dBi and 7.9 dBi, respectively, have been achieved. The measured results of the prototype gave two bands extending from 3.55 to 13.05 GHz (114.46%) and from 14.3 to 16 GHz (11%).

ACKNOWLEDGMENT

This work has received funding from the European Union’s Horizon 2020 research and innovation program under grant agreement H2020-MSCA-ITN-2016 SECRET-722424. This work is also funded by the FCT / MEC through national funds and when applicable co-financed by the ERDF, under the PT2020 Partnership Agreement under the UID / EEA / 50008/2019 project.

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